National Semiconductor

LMC6062 Precision CMOS Dual Micropower Operational Amplifier

General Description

The LMC6062 is a precision dual low offset voltage, micropower operational amplifier, capable of precision single supply operation. Performance characteristics include ultra low input bias current, high voltage gain, rail-to-rail output swing, and an input common mode voltage range that includes ground. These features, plus its low power consumption, make the LMC6062 ideally suited for battery powered applications.

Other applications using the LMC6062 include precision full-wave rectifiers, integrators, references, sample-and-hold circuits, and true instrumentation amplifiers.

This device is built with National's advanced double-Poly Silicon-Gate CMOS process.

For designs that require higher speed, see the LMC6082 precision dual operational amplifier.

PATENT PENDING

Features (Typical Unless Otherwise Noted)

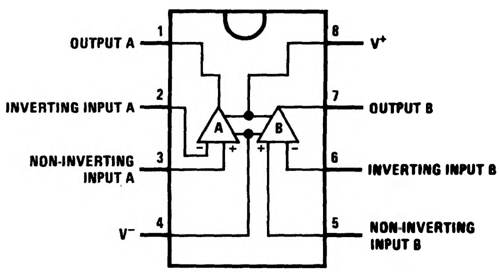
- Low offset voltage 100 μV
- Ultra low supply current 16 μA/Amplifier
- Operates from 4.5V to 15V single supply
- Ultra low input bias current 10 fA
- Output swing within 10 mV of supply rail, 100k load
- Input common-mode range includes V^-
- High voltage gain 140 dB
- Improved latchup immunity

Applications

- Instrumentation amplifier
- Photodiode and infrared detector preamplifier
- Transducer amplifiers
- Hand-held analytic instruments
- Medical instrumentation
- D/A converter
- Charge amplifier for piezoelectric transducers

Connection Diagram

8-Pin DIP/SO



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Top View

Ordering Information

Package	Temperature Range		NSC Drawing	Transport Media
	Military −55°C to +125°C	Industrial −40°C to +85°C		
8-Pin Molded DIP	LMC6062AMN	LMC6062AIN LMC6062IN	N08E	Rail
8-Pin Small Outline		LMC6062AIM LMC6062IM	M08A	Rail Tape and Reel
8-Pin Ceramic DIP	LMC6062AMJ/883		J08A	Rail

Absolute Maximum Ratings (Note 1)

If Military/Aerospace specified devices are required, please contact the National Semiconductor Sales Office/Distributors for availability and specifications.

Differential Input Voltage	±Supply Voltage
Voltage at Input/Output Pin	(V+) +0.3V, (V−) −0.3V
Supply Voltage (V+ − V−)	16V
Output Short Circuit to V+	(Note 11)
Output Short Circuit to V−	(Note 2)
Lead Temperature (Soldering, 10 sec.)	260°C
Storage Temp. Range	−65°C to +150°C
Junction Temperature	150°C
ESD Tolerance (Note 4)	2 kV
Current at Input Pin	±10 mA
Current at Output Pin	±30 mA
Current at Power Supply Pin	40 mA
Power Dissipation	(Note 3)

Operating Ratings (Note 1)

Temperature Range	
LMC6062AM	$-55°C \leq T_J \leq +125°C$
LMC6062AI, LMC6082I	$-40°C \leq T_J \leq +85°C$
Supply Voltage	$4.5V \leq V^+ \leq 15.5V$
Thermal Resistance (θ_{JA}) (Note 12)	
8-Pin Molded DIP	115°C/W
8-Pin SO	193°C/W
Power Dissipation	(Note 10)

DC Electrical Characteristics

Unless otherwise specified, all limits guaranteed for $T_J = 25°C$. **Boldface** limits apply at the temperature extremes. $V^+ = 5V$, $V^- = 0V$, $V_{CM} = 1.5V$, $V_O = 2.5V$ and $R_L > 1M$ unless otherwise specified.

Symbol	Parameter	Conditions		Typ (Note 5)	LMC6062AM Limit (Note 6)	LMC6062AI Limit (Note 6)	LMC6062I Limit (Note 6)	Units
V_{OS}	Input Offset Voltage			100	350 **1200**	350 **900**	800 **1300**	µV Max
TCV_{OS}	Input Offset Voltage Average Drift			1.0				µV/°C
I_B	Input Bias Current			0.010	**100**	**4**	**4**	pA Max
I_{OS}	Input Offset Current			0.005	**100**	**2**	**2**	pA Max
R_{IN}	Input Resistance			>10				Tera Ω
CMRR	Common Mode Rejection Ratio	$0V \leq V_{CM} \leq 12.0V$ $V^+ = 15V$		85	75 **70**	75 **72**	66 **63**	dB Min
+PSRR	Positive Power Supply Rejection Ratio	$5V \leq V^+ \leq 15V$ $V_O = 2.5V$		85	75 **70**	75 **72**	66 **63**	dB Min
−PSRR	Negative Power Supply Rejection Ratio	$0V \leq V^- \leq -10V$		100	84 **70**	84 **81**	74 **71**	dB Min
V_{CM}	Input Common-Mode Voltage Range	$V^+ = 5V$ and 15V for CMRR ≥ 60 dB		−0.4	−0.1 **0**	−0.1 **0**	−0.1 **0**	V Max
				$V^+ - 1.9$	$V^+ - 2.3$ **$V^+ - 2.6$**	$V^+ - 2.3$ **$V^+ - 2.5$**	$V^+ - 2.3$ **$V^+ - 2.5$**	V Min
A_V	Large Signal Voltage Gain	$R_L = 100\ k\Omega$ (Note 7)	Sourcing	4000	400 **200**	400 **300**	300 **200**	V/mV Min
			Sinking	3000	180 **70**	180 **100**	90 **60**	V/mV Min
		$R_L = 25\ k\Omega$ (Note 7)	Sourcing	3000	400 **150**	400 **150**	200 **80**	V/mV Min
			Sinking	2000	100 **35**	100 **50**	70 **35**	V/mV Min

DC Electrical Characteristics (Continued)

Unless otherwise specified, all limits guaranteed for $T_J = 25°C$. **Boldface** limits apply at the temperature extremes. $V^+ = 5V$, $V^- = 0V$, $V_{CM} = 1.5V$, $V_O = 2.5V$ and $R_L > 1M$ unless otherwise specified.

Symbol	Parameter	Conditions	Typ (Note 5)	LMC6062AM Limit (Note 6)	LMC6062AI Limit (Note 6)	LMC6062I Limit (Note 6)	Units
V_O	Output Swing	$V^+ = 5V$ $R_L = 100\ k\Omega$ to 2.5V	4.995	4.990 **4.970**	4.990 **4.980**	4.950 **4.925**	V Min
			0.005	0.010 **0.030**	0.010 **0.020**	0.050 **0.075**	V Max
		$V^+ = 5V$ $R_L = 25\ k\Omega$ to 2.5V	4.990	4.975 **4.955**	4.975 **4.965**	4.950 **4.850**	V Min
			0.010	0.020 **0.045**	0.020 **0.035**	0.050 **0.150**	V Max
		$V^+ = 15V$ $R_L = 100\ k\Omega$ to 7.5V	14.990	14.975 **14.955**	14.975 **14.965**	14.950 **14.925**	V Min
			0.010	0.025 **0.050**	0.025 **0.035**	0.050 **0.075**	V Max
		$V^+ = 15V$ $R_L = 25\ k\Omega$ to 7.5V	14.965	14.900 **14.800**	14.900 **14.850**	14.850 **14.800**	V Min
			0.025	0.050 **0.200**	0.050 **0.150**	0.100 **0.200**	V Max
I_O	Output Current $V^+ = 5V$	Sourcing, $V_O = 0V$	22	16 **8**	16 **10**	13 **8**	mA Min
		Sinking, $V_O = 5V$	21	16 **7**	16 **8**	16 **8**	mA Min
I_O	Output Current $V^+ = 15V$	Sourcing, $V_O = 0V$	25	15 **9**	15 **10**	15 **10**	mA Min
		Sinking, $V_O = 13V$ (Note 11)	35	24 **7**	24 **8**	24 **8**	mA Min
I_S	Supply Current	Both Amplifiers $V^+ = +5V$, $V_O = 1.5V$	32	38 **60**	38 **46**	46 **56**	μA Max
		Both Amplifiers $V^+ = +15V$, $V_O = 7.5V$	40	47 **70**	47 **55**	57 **66**	μA Max

AC Electrical Characteristics

Unless otherwise specified, all limits guaranteed for $T_J = 25°C$, **Boldface** limits apply at the temperature extremes. $V^+ = 5V$, $V^- = 0V$, $V_{CM} = 1.5V$, $V_O = 2.5V$ and $R_L > 1M$ unless otherwise specified.

Symbol	Parameter	Conditions	Typ (Note 5)	LMC6062AM Limit (Note 6)	LMC6062AI Limit (Note 6)	LMC6062I Limit (Note 6)	Units
SR	Slew Rate	(Note 8)	35	20 **8**	20 **10**	15 **7**	V/ms Min
GBW	Gain-Bandwidth Product		100				kHz
θ_m	Phase Margin		50				Deg
	Amp-to-Amp Isolation	(Note 9)	155				dB
e_n	Input-Referred Voltage Noise	F = 1 kHz	83				$nV/\sqrt{Hz}$
i_n	Input-Referred Current Noise	F = 1 kHz	0.0002				$pA/\sqrt{Hz}$
T.H.D.	Total Harmonic Distortion	F = 1 kHz, $A_V = -5$ $R_L = 100\ k\Omega$, $V_O = 2\ V_{PP}$ ±5V Supply	0.01				%

Note 1: Absolute Maximum Ratings indicate limits beyond which damage to the device may occur. Operating Ratings indicate conditions for which the device is intended to be functional, but do not guarantee specific performance limits. For guaranteed specifications and test conditions, see the Electrical Characteristics. The guaranteed specifications apply only for the test conditions listed.

Note 2: Applies to both single-supply and split-supply operation. Continous short circuit operation at elevated ambient temperature can result in exceeding the maximum allowed junction temperature of 150°C. Output currents in excess of ±30 mA over long term may adversely affect reliability.

Note 3: The maximum power dissipation is a function of $T_{J(Max)}$, θ_{JA}, and T_A. The maximum allowable power dissipation at any ambient temperature is $P_D = (T_{J(Max)} - T_A)/\theta_{JA}$.

Note 4: Human body model, 1.5 kΩ in series with 100 pF.

Note 5: Typical values represent the most likely parametric norm.

Note 6: All limits are guaranteed by testing or statistical analysis.

Note 7: $V^+ = 15V$, $V_{CM} = 7.5V$ and R_L connected to 7.5V. For Sourcing tests, $7.5V \leq V_O \leq 11.5V$. For Sinking tests, $2.5V \leq V_O \leq 7.5V$.

Note 8: $V^+ = 15V$. Connected as Voltage Follower with 10V step input. Number specified is the slower of the positive and negative slew rates.

Note 9: Input referred $V^+ = 15V$ and $R_L = 100\ k\Omega$ connected to 7.5V. Each amp excited in turn with 100 Hz to produce $V_O = 12\ V_{PP}$.

Note 10: For operating at elevated temperatures the device must be derated based on the thermal resistance θ_{JA} with $P_D = (T_J - T_A)/\theta_{JA}$.

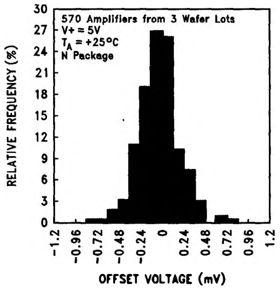
Note 11: Do not connect output to V^+, when V^+ is greater than 13V or reliability witll be adversely affected.

Note 12: All numbers apply for packages soldered directly into a PC board.

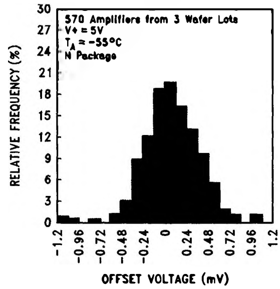
Note 13: For guaranteed Military Temperature Range parameters, see RETSMC6062X.

Typical Performance Characteristics $V_S = \pm 7.5V$, $T_A = 25°C$, Unless otherwise specified

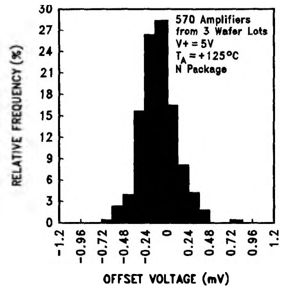
Distribution of LMC6062 Input Offset Voltage ($T_A = +25°C$)



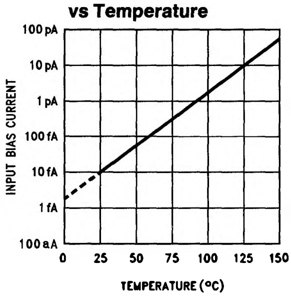
Distribution of LMC6062 Input Offset Voltage ($T_A = -55°C$)



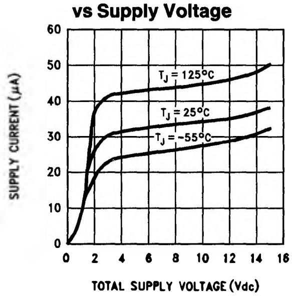
Distribution of LMC6062 Input Offset Voltage ($T_A = +125°C$)



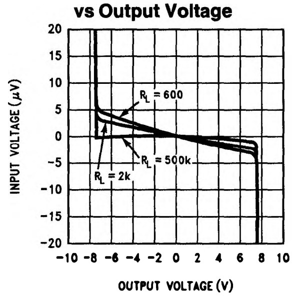
Input Bias Current vs Temperature



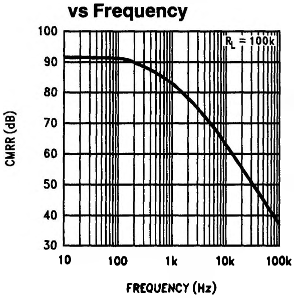
Supply Current vs Supply Voltage



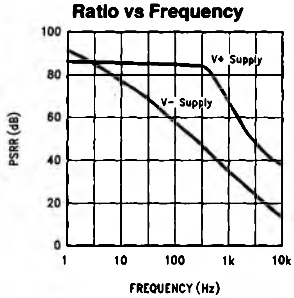
Input Voltage vs Output Voltage



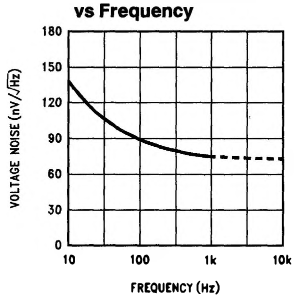
Common Mode Rejection Ratio vs Frequency



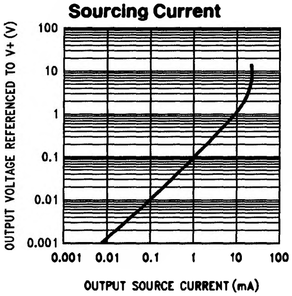
Power Supply Rejection Ratio vs Frequency



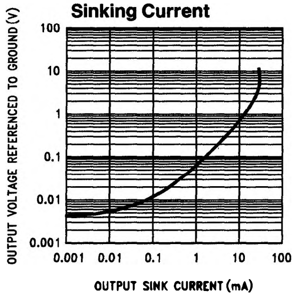
Input Voltage Noise vs Frequency



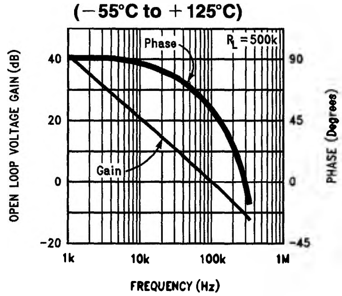
Output Characteristics Sourcing Current



Output Characteristics Sinking Current



Gain and Phase Response vs Temperature (−55°C to +125°C)



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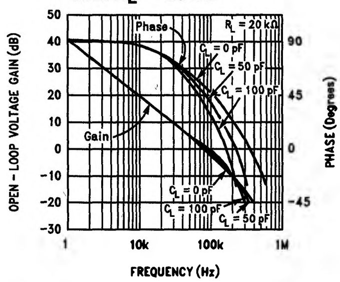
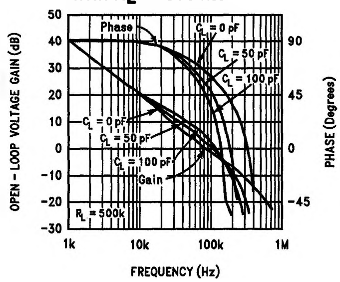
Typical Performance Characteristics $V_S = \pm 7.5V$, $T_A = 25°C$, Unless otherwise specified

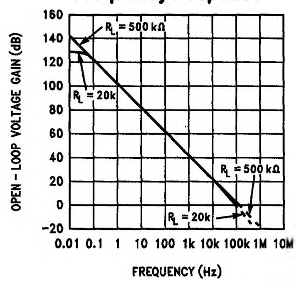
Gain and Phase Response vs Capacitive Load with $R_L = 20\ k\Omega$



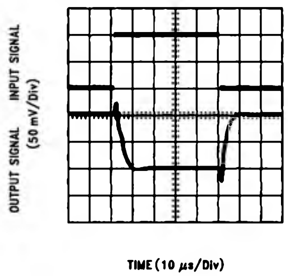
Gain and Phase Response vs Capacitive Load with $R_L = 500\ k\Omega$



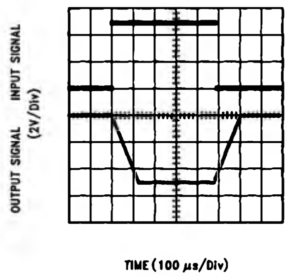
Open Loop Frequency Response



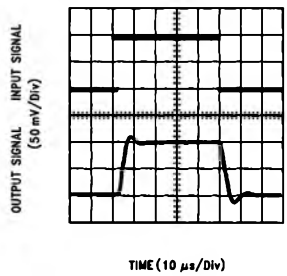
Inverting Small Signal Pulse Response



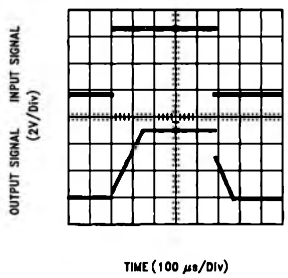
Inverting Large Signal Pulse Response



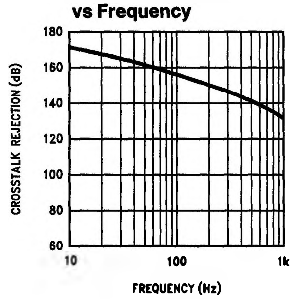
Non-Inverting Small Signal Pulse Response



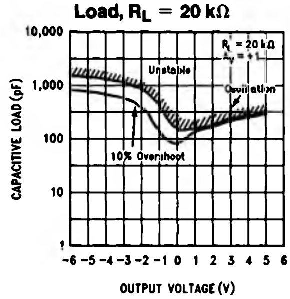
Non-Inverting Large Signal Pulse Response



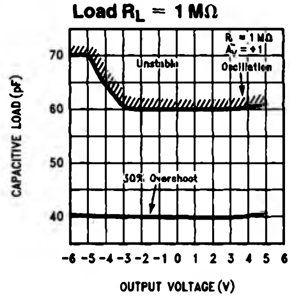
Crosstalk Rejection vs Frequency



Stability vs Capacitive Load, $R_L = 20\ k\Omega$



Stability vs Capacitive Load $R_L = 1\ M\Omega$



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Applications Hints

AMPLIFIER TOPOLOGY

The LMC6062 incorporates a novel op-amp design topology that enables it to maintain rail-to-rail output swing even when driving a large load. Instead of relying on a push-pull unity gain output buffer stage, the output stage is taken directly from the internal integrator, which provides both low output impedance and large gain. Special feed-forward compensation design techniques are incorporated to maintain stability over a wider range of operating conditions than traditional micropower op-amps. These features make the LMC6062 both easier to design with, and provide higher speed than products typically found in this ultra-low power class.

COMPENSATING FOR INPUT CAPACITANCE

It is quite common to use large values of feedback resistance for amplifiers with ultra-low input current, like the LMC6062.

Although the LMC6062 is highly stable over a wide range of operating conditions, certain precautions must be met to achieve the desired pulse response when a large feedback resistor is used. Large feedback resistors and even small values of input capacitance, due to transducers, photodiodes, and circuit board parasitics, reduce phase margins.

When high input impedances are demanded, guarding of the LMC6062 is suggested. Guarding input lines will not only reduce leakage, but lowers stray input capacitance as well. (See ***Printed-Circuit-Board Layout for High Impedance Work***).

The effect of input capacitance can be compensated for by adding a capacitor. Place a capacitor, C_f, around the feedback resistor (as in *Figure 1*) such that:

$$\frac{1}{2\pi R_1 C_{IN}} \geq \frac{1}{2\pi R_2 C_f}$$

or

$$R_1 C_{IN} \leq R_2 C_f$$

Since it is often difficult to know the exact value of C_{IN}, C_f can be experimentally adjusted so that the desired pulse response is achieved. Refer to the LMC660 and the LMC662 for a more detailed discussion on compensating for input capacitance.

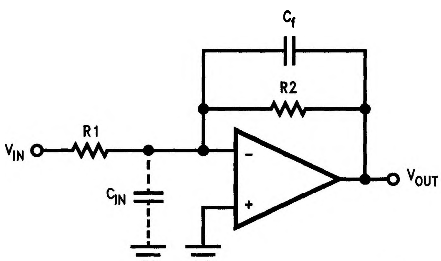

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FIGURE 1. Canceling the Effect of Input Capacitance

CAPACITIVE LOAD TOLERANCE

All rail-to-rail output swing operational amplifiers have voltage gain in the output stage. A compensation capacitor is normally included in this integrator stage. The frequency location of the dominate pole is affected by the resistive load on the amplifier. Capacitive load driving capability can be optimized by using an appropriate resistive load in parallel with the capacitive load (see typical curves).

Direct capacitive loading will reduce the phase margin of many op-amps. A pole in the feedback loop is created by the combination of the op-amp's output impedance and the capacitive load. This pole induces phase lag at the unity-gain crossover frequency of the amplifier resulting in either an oscillatory or underdamped pulse response. With a few external components, op amps can easily indirectly drive capacitive loads, as shown in *Figure 2a*.

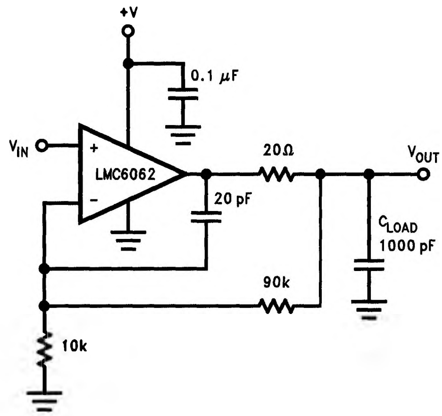

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FIGURE 2a. LMC6062 Noninverting Gain of 10 Amplifier, Compensated to Handle Capacitive Loads

In the circuit of *Figure 2a*, R1 and C1 serve to counteract the loss of phase margin by feeding the high frequency component of the output signal back to the amplifier's inverting input, thereby preserving phase margin in the overall feedback loop.

Capacitive load driving capability is enhanced by using a pull up resistor to V^+ *(Figure 2b)*. Typically a pull up resistor conducting 10 μA or more will significantly improve capacitive load responses. The value of the pull up resistor must be determined based on the current sinking capability of the amplifier with respect to the desired output swing. Open loop gain of the amplifier can also be affected by the pull up resistor (see Electrical Characteristics).

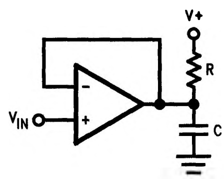

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FIGURE 2b. Compensating for Large Capacitive Loads with a Pull Up Resistor

PRINTED-CIRCUIT-BOARD LAYOUT FOR HIGH-IMPEDANCE WORK

It is generally recognized that any circuit which must operate with less than 1000 pA of leakage current requires special layout of the PC board. When one wishes to take advantage of the ultra-low bias current of the LMC6062, typically less than 10 fA, it is essential to have an excellent layout. Fortunately, the techniques of obtaining low leakages are

Applications Hints (Continued)

quite simple. First, the user must not ignore the surface leakage of the PC board, even though it may sometimes appear acceptably low, because under conditions of high humidity or dust or contamination, the surface leakage will be appreciable.

To minimize the effect of any surface leakage, lay out a ring of foil completely surrounding the LMC6062's inputs and the terminals of capacitors, diodes, conductors, resistors, relay terminals etc. connected to the op-amp's inputs, as in *Figure 3*. To have a significant effect, guard rings should be placed on both the top and bottom of the PC board. This PC foil must then be connected to a voltage which is at the same voltage as the amplifier inputs, since no leakage current can flow between two points at the same potential. For example, a PC board trace-to-pad resistance of $10^{12}\Omega$, which is normally considered a very large resistance, could leak 5 pA if the trace were a 5V bus adjacent to the pad of the input. This would cause a 100 times degradation from the LMC6062's actual performance. However, if a guard ring is held within 5 mV of the inputs, then even a resistance of $10^{11}\Omega$ would cause only 0.05 pA of leakage current. See *Figures 4a, 4b, 4c* for typical connections of guard rings for standard op-amp configurations.

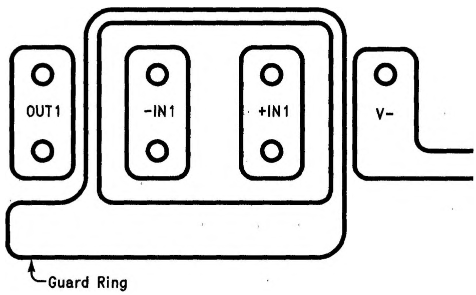

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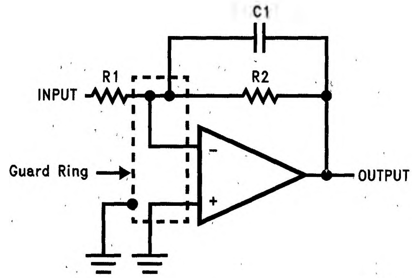
FIGURE 3. Example of Guard Ring in P.C. Board Layout



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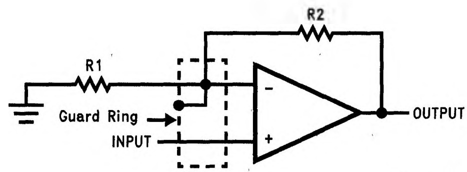
(a) Inverting Amplifier



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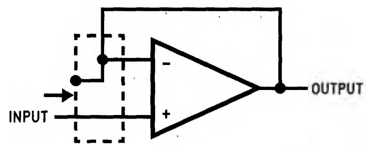
(b) Non-Inverting Amplifier



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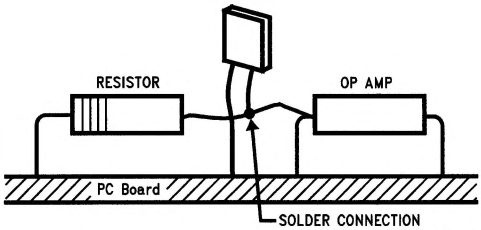
(c) Follower

FIGURE 4. Typical Connections of Guard Rings

The designer should be aware that when it is inappropriate to lay out a PC board for the sake of just a few circuits, there is another technique which is even better than a guard ring on a PC board: Don't insert the amplifier's input pin into the board at all, but bend it up in the air and use only air as an insulator. Air is an excellent insulator. In this case you may have to forego some of the advantages of PC board construction, but the advantages are sometimes well worth the effort of using point-to-point up-in-the-air wiring. See *Figure 5*.

Latchup

CMOS devices tend to be susceptible to latchup due to their internal parasitic SCR effects. The (I/O) input and output pins look similar to the gate of the SCR. There is a minimum current required to trigger the SCR gate lead. The LMC6062 and LMC6082 are designed to withstand 100 mA surge current on the I/O pins. Some resistive method should be used to isolate any capacitance from supplying excess current to the I/O pins. In addition, like an SCR, there is a minimum holding current for any latchup mode. Limiting current to the supply pins will also inhibit latchup susceptibility.



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(Input pins are lifted out of PC board and soldered directly to components. All other pins connected to PC board).

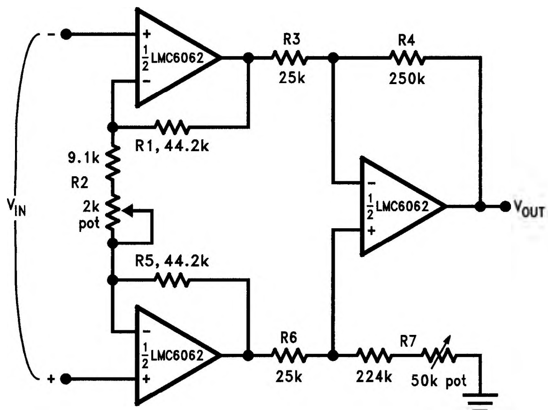
FIGURE 5. Air Wiring

Typical Single-Supply Applications

($V^{+} = 5.0\ V_{DC}$)

The extremely high input impedance, and low power consumption, of the LMC6062 make it ideal for applications that require battery-powered instrumentation amplifiers. Examples of these types of applications are hand-held pH probes, analytic medical instruments, magnetic field detectors, gas detectors, and silicon based pressure transducers.

Figure 6 shows an instrumentation amplifier that features high differential and common mode input resistance ($>10^{14}\Omega$), 0.01% gain accuracy at $A_V = 100$, excellent CMRR with 1 kΩ imbalance in bridge source resistance. Input current is less than 100 fA and offset drift is less than 2.5 μV/°C. R_2 provides a simple means of adjusting gain over a wide range without degrading CMRR. R_7 is an initial trim used to maximize CMRR without using super precision matched resistors. For good CMRR over temperature, low drift resistors should be used.



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If $R_1 = R_5$, $R_3 = R_6$, and $R_4 = R_7$; then

$$\frac{V_{OUT}}{V_{IN}} = \frac{R_2 + 2R_1}{R_2} \times \frac{R_4}{R_3}$$

$\therefore A_V \approx 100$ for circuit shown ($R_2 = 9.822k$).

FIGURE 6. Instrumentation Amplifier

Typical Single-Supply Applications ($V^+ = 5.0\ V_{DC}$) (Continued)

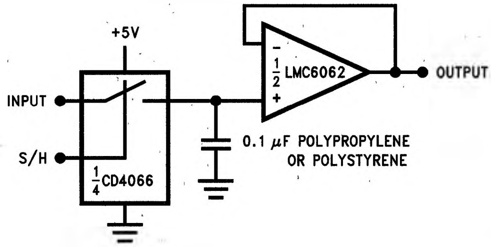

FIGURE 7. Low-Leakage Sample and Hold

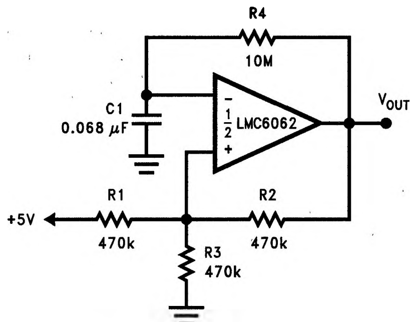

FIGURE 8. 1 Hz Square Wave Oscillator